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High Accuracy Microwave Frequency Measurement Based on Single-Drive Dual-Parallel Mach-Zehnder Modulator

Ying Zhao^{1,2†}, Lei Deng^{2,3}, Xiaodan Pang², Xianbin Yu², Xiaoping Zheng^{1‡},
Bingkun Zhou¹ and I. Tafur Monroy²

¹Department of Electronic Engineering, Tsinghua National Laboratory for Information Science and Technology, Tsinghua University, 100084 Beijing, China.

²DTU Fotonik, Technical University of Denmark, DK-2800, Kgs. Lyngby, Denmark.

³School of Optoelectronics Science & Engineering, HuaZhong University of Science & Technology, Wuhan, China.
†yinzhang@fotonik.dtu.dk ‡xpxzheng@mail.tsinghua.edu.cn

Abstract: A novel approach for broadband microwave frequency measurement based on bias manipulation of a dual-parallel Mach-Zehnder modulator is proposed and experimentally demonstrated. A 10^{-3} relative error verifies a significant accuracy improvement by this method.

OCIS codes: (060.5625) Radio frequency photonics, (350.4010) Microwaves.

1. Introduction

Microwave photonics has driven and facilitated various kinds of applications for its superiority on potential high-speed and parallel microwave signal processing capability [1]. For electronic warfare and defense applications, carrier frequency measurement in optical manners can be a promising solution for intercepted signal processing where a high accuracy and large measurement range is required. The primary advantages of photonics-assisted microwave frequency measurement are the broadband and real-time operation of lightwave signals. Generally, the frequency measurement can be realized by comparing the power of two microwave signals experiencing different dispersion-induced fading effects in the optical link. Recently, the frequency-to-power mapping technique has been proposed and investigated by different methods [2–4]. Complementary filtering implemented by microwave photonic filters [2] are generally adopted while other schemes using multiple laser sources or modulators are developed [3, 4]. The major limitation of previous methods is the comparatively large relative measurement error (several percent), which prevents them from being used in high accuracy applications.

In this paper, we propose and demonstrate a novel approach for high accuracy frequency measurement using a single-drive dual parallel Mach-Zehnder modulator (SD-DPMZM). By tuning one of the bias points of the SD-DPMZM, the power fading characteristics of the unknown microwave signal changes, which thereby results in the change of measurement accuracy. Therefore, the highest accuracy point can be obtained by flexible manipulating the modulator bias point. The experiment verifies the improved accuracy of this approach by performing a $\sim 10^{-3}$ relative error within a 10GHz measurement range.

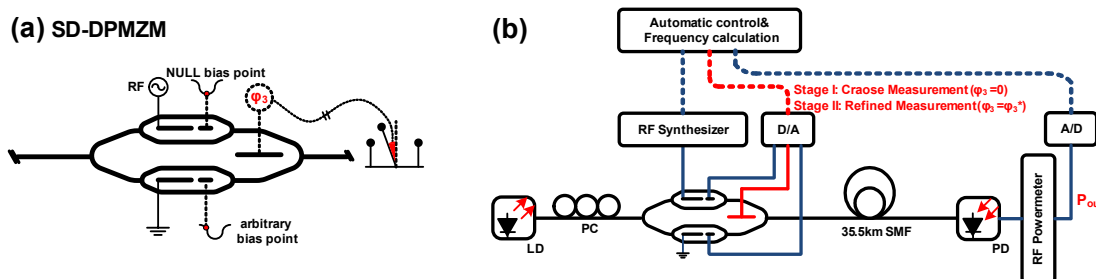


Fig. 1. (a) Bias arrangement of a SD-MZM for frequency measurement. (b) Experimental setup of a high accuracy frequency measurement system. LD: laser diode. PC: polarization controller. PD: photodiode. A/D and D/A: analog to digital converter and digital to analog converter.

2. Principle

Fig.1(a) shows the bias arrangement of a DPMZM for frequency measurement purpose. The structure of the DPMZM contains two sub-MZMs, MZM1 and MZM2, lying in parallel on two arms of MZM3, which controlled only by its bias voltage without drive. In our case, MZM1 is biased at the minimal transmission point (NULL point) and driven by the unknown RF signal to perform carrier suppressed double sideband (CSDSB) modulation. MZM2 is remained un-modulated and arbitrarily biased to let the optical carrier propagate through. This asymmetrical arrangement is named single-drive of a DPMZM or CSDSB+Carrier modulation scheme [5]. The phase difference φ_3 between the optical carrier and two first-order sidebands is determined by the bias point of the MZM3, which also gives a RF φ_3 -dependent power fading after dispersive transmission. As shown in Fig.1(b), the output RF power can be given by

$$P_{out}(\varphi_3) \propto \cos^2\left(\frac{\beta_2 \cdot L}{2}\Omega^2 + \varphi_3\right) \quad (1)$$

where β_2 and L are the dispersion coefficient and the length of the dispersive link, respectively. Ω is the angular frequency of the unknown RF signal. To eliminate undesirable effects caused by the non-flat frequency response of components in the link, a relative power comparison function (PCF) is introduced to construct RF frequency-to-power mapping, which can be expressed as $PCF(\varphi_3) = P_{out}(\varphi_3|_{t_1})/P_{out}(\varphi_3|_{t_2} = \varphi_3|_{t_1} + \frac{\pi}{2})$, where $\varphi_3|_{t_1}$ and $\varphi_3|_{t_2}$ are bias phases of twice measurements at time t_1 and t_2 and the phase difference between these measurements is fixed at $\pi/2$. Therefore the unknown frequency is determined by

$$\Omega(\varphi_3|_{t_1}) = \sqrt{\frac{2(\arccot(\sqrt{PCF}) - \varphi_3|_{t_1})}{\beta_2 \cdot L}} \quad (2)$$

Since φ_3 is an inherent parameter of the DPMZM and only dependent on the bias of the MZM3, we can flexibly choose $\varphi_3|_{t_1}$ to achieve a potential high accuracy point implied by Eq.(2). If we choose the bias point

$$\varphi_3^*|_{t_1} = -\frac{\beta_2 \cdot L}{2}\Omega^2 \quad (3)$$

the derivative $\frac{\partial \Omega}{\partial PCF}|_{\varphi_3^*} = 0$, which means the measurement frequency is non-sensitive to PCF error at all. The highest accuracy can be achieved by this deliberate bias manipulation.

3. Experimental setup

Fig.1(b) shows the high accuracy frequency measurement system using the proposed approach. The unknown RF signal is modulated onto an optical carrier at 1549.8nm based on a SD-DPMZM. The optical signal is launched into a 35.5km single mode fiber (SMF) and then detected by a photodiode. The power of the dispersion-induced fading signal is monitored by a RF powermeter. The system is running automatically by employing program-based GPIB instrument control interface implemented in MATLAB. The frequency measurement procedure is divided into two stages, I) the coarse measurement and II) the accuracy refining measurement. In the stage I, the coarse frequency $\tilde{\Omega}$ is estimated based on Eq.(2) with the fixed bias phase $\varphi_3 = 0$, which means the high accuracy requirement (Eq.(3)) is not satisfied in this case. The main purpose of the coarse measurement stage is to lead the bias point to approach the requirement of Eq.(3) in the stage II. By using the coarse measured frequency $\tilde{\Omega}$, we can approximately calculate the bias point φ_3^* for highest accuracy using Eq.(3). The measurement system then switches the DC bias of the MZM3 to φ_3^* and refines the measurement process. In our experiment, the stage II is executed iteratively for ten times and the output values are averaged as the final frequency estimation.

4. Experimental results

Fig.2 shows the coarse measurement results with φ_3 fixed at 0. The PCF value with respect to the reference frequencies for different RF input powers is shown in Fig.2(a). The first power fading notch is at ~ 10 GHz, which implies the unambiguous frequency measurement range is ~ 10 GHz. This range can be adjusted by changing the amount of the optical link dispersion. Fig.2(b) shows the measured frequencies obtained from Eq.(2) as well as reference frequencies for different input power levels. The errors between the measurement and the reference are shown in Fig.2(c). The error curve drops significantly when the reference frequency is close to 10GHz because for a 35.5km SMF, the highest accuracy requirement of the bias point is $\varphi_3^* \doteq 0$, almost got satisfied in the coarse measurement case. Fig.3 shows the high accuracy measurement results based on the coarse pre-measurement for a 10dBm RF input. Fig.3(a) shows the error limits of the ten times iterative refined measurements. The absolute error fluctuation is less than 5MHz, which shows the stability of the refined measurement process. The absolute error comparison between the coarse and refined measurements is shown in Fig.3(b). By performing high accuracy measurement, the average uncertainty

of the measured frequency can be tremendously decreased from 118MHz to 5.4MHz. Fig.3(c) shows the refined measurement error with the MZM3 bias voltage drift for 10GHz reference frequency considering the non-ideal biasing characteristics of the DPMZM. In this case, the bias drift is emulated by intentionally inducing a deviation from ϕ_3^* . A $\sim 60\text{MHz/V}$ degradation of measurement performance is observed.

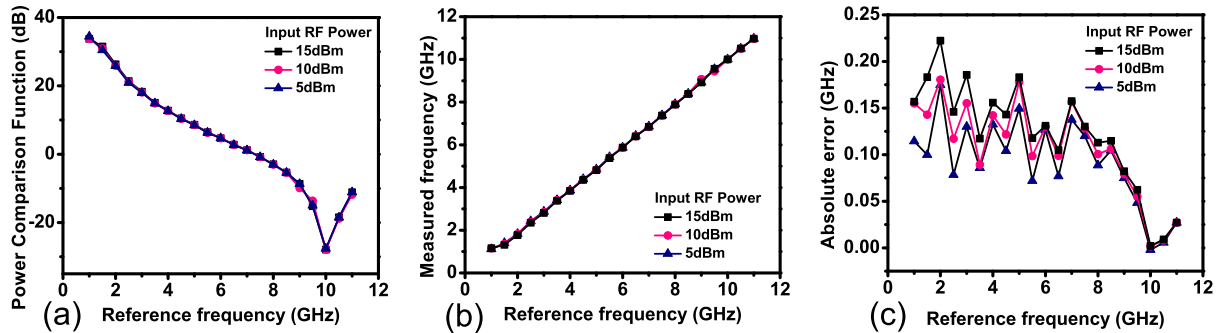


Fig. 2. Frequency measurement results of coarse stage. (a) PCF value versus input RF frequency for different RF power. (b) Measured RF frequency versus input reference frequency for different RF power. (c) Absolute measurement error versus input reference frequency for different RF power.

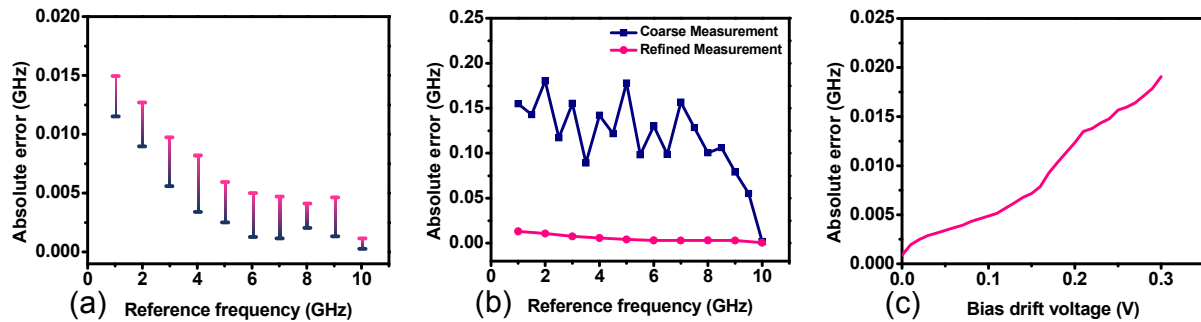


Fig. 3. Frequency measurement results of refined stage. (a) Error range for ten times refined measurements. (b) Error comparison of coarse and refined measurement. (c) Absolute error effected by the MZM3 bias drift.

5. Conclusions

A novel scheme for high accuracy broadband microwave frequency measurement is proposed, theoretically analyzed and experimentally demonstrated. By using a SD-DPMZM and performing a two-stage measurement, this method shows an improved relative error of 10^{-3} .

6. Acknowledgements

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